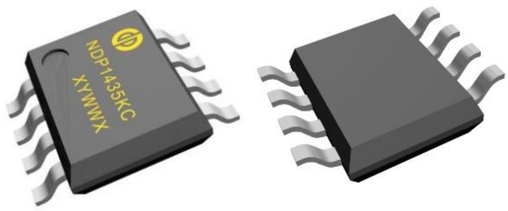
3.5A,40V High Efficiency Synchronous Step-Down DC/DC Converter

Description

NDP1435KC is a high efficiency, monolithic synchronous step-down DC/DC converter utilizing a constant frequency, average current mode control architecture. Capable of delivering up to 3.5A continuous load with excellent line and load regulation. The device operates from an input voltage range of 7V to 38V and provides an adjustable output voltage from 3.6V to 25V.

The NDP1435KC features short circuit and thermal protection circuits to increase system reliability. The internal soft start avoids input inrush current during startup.

The NDP1435KC require a minimum number of external components. and a wide array of protection features to enhance reliability.



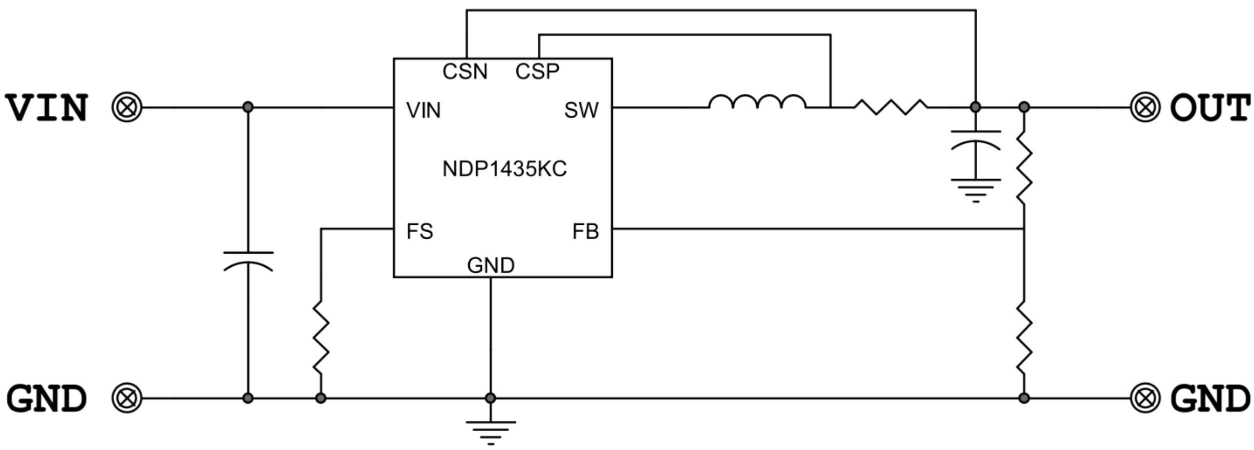
Features

- VIN Range: 7V to 38V
- 3.5A Continuous Output Current
- Up to 94% Efficiency
- CC/CV Mode Control
- 100% Max Duty Cycle
- Built in Adjustable Line-Compensation
- Adjustable Output Voltages
- Output Voltage Accuracy: +/-1.5%
- Current Limit Accuracy: +/- 5%
- Integrated 45mΩ High Side Switch
- Integrated 23mΩ Low Side Switch
- Programable Frequency:130kHz~300kHz
- Burst Mode Operation at Light Load
- Internal loop Compensation
- Internal Soft Start
- Available in SOP8 Package

Applications

- Car Charger
- Rechargeable Portable Devices
- Networking Systems
- Distributed Power Systems

Typical Application

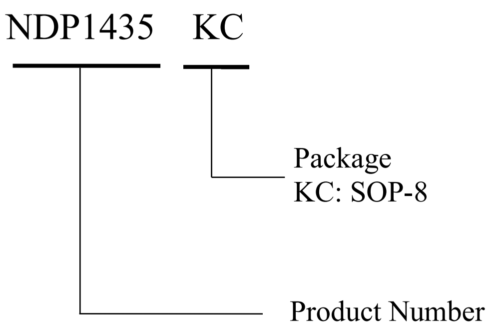


Note: When using a solid or ceramic input Cap, It is recommended to parallel a TVS diode.

Order Information

Orderable Device	Package Type	Packing Qty/reel	MSL- Peak Temp -Floor Life	Eco Std	Marking Information
NDP1435KC	SOP8	4000	MSL3-260℃-168hrs	RoHS & Green	Refer to below

Product Naming



Top Side Marking

X: Internal ID Code
YY: Year (2=2022,3=2023,…)
WW: Weekly (01-53)

Notes:

(1) **RoHS**: Quoted from **RoHS Detective (EU) 2015/863**, Deep-Pool defines "RoHS" to mean semiconductor products that are compliant with the current EU RoHS requirements. Where designed to be soldered at high temperatures, "RoHS" products are suitable for use in specified lead-free processes. Deep-Pool may reference these types of products as "**Pb-Free**".

(2) **RoHS Exempt:** Deep-Pool defines "RoHS Exempt" to mean products that contain lead but are compliant with EU RoHS pursuant to a specific EU RoHS exemption.

(3) **Green**: Deep-Pool defines "Green" to mean the content of Chlorine (Cl) and Bromine (Br) based flame retardants meet JEDEC (**JS709C**) low halogen requirements of <=1000ppm threshold.

(4) **MSL**, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC (**J-STD-020F**) industry standard classifications, as well as the peak solder temperature of SMT and the floor life after unpacking, which customers should pay attention and strictly comply with the standard to use.

(5) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

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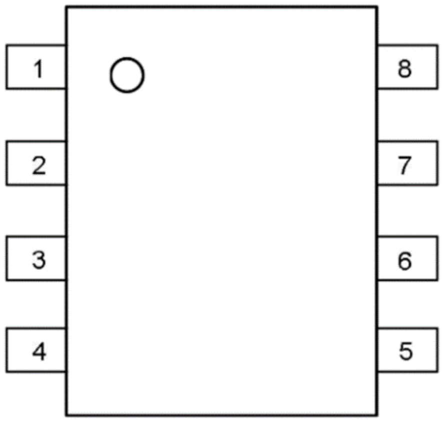
Pin Function and Definition

PIN	NAME	Description
1	VFB	Feedback of Output Voltage
2	CSP	Positive Pole of Current Sense
3	CSN	Negative Pole1 of Current Sense
4	VIN	Power Input Positive Pole
5,6	SW	Switching, Connected with an Inductor
7	FS	Connect a Resistor to GND for Frequency Config
8	GND	Ground



Absolute Maximum Ratings (at TA = 25°C)

Characteristics	Symbol	Rating	Unit
VIN to GND		-0.3 to 44	V
SW to GND		-0.3 to VIN+0.3	V
FB, FS to GND		-0.3 to 6	V
CSP, CSN to GND		-0.3 to 25	V
Operating Junction Temperature	T_A	-40 to 150	°C
Storage Junction Temperature	Tstg	-65 to 150	°C
Thermal Resistance from Junction to case	θ_{JC}	45	°C/W
Thermal Resistance from Junction to ambient	θ_{JA}	90	°C/W

Notes:

Stresses at or above those listed under Absolute Maximum Ratings may cause permanent damage to the product. This is a stress rating only; functional operation of the product at these or any other conditions above those indicated in the operational section of this specification is not implied. Operation beyond the maximum operating conditions for extended periods may affect product reliability.

Recommended Operating Range

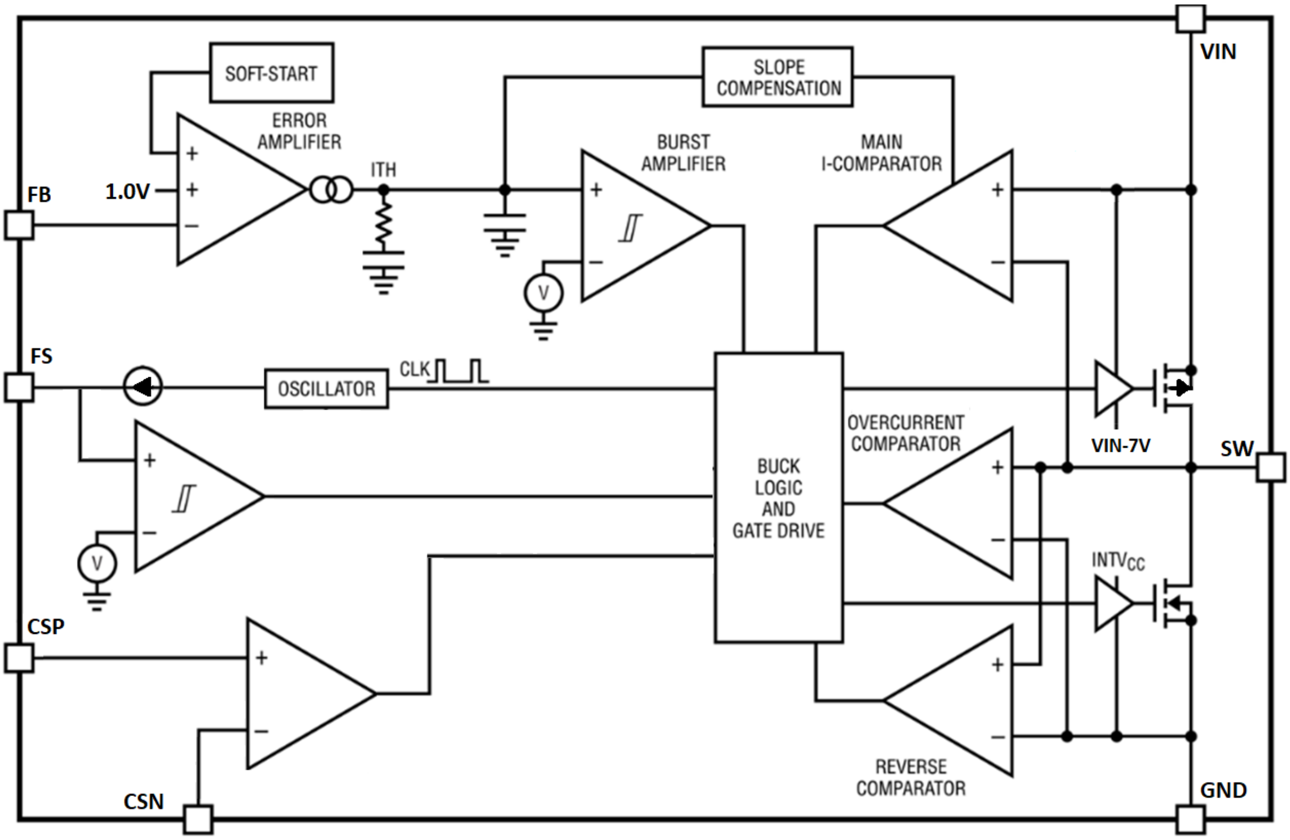
ELECTRICAL PARAMETER	MINIMUM	TYPICAL	MAXIMUM	UNIT
Input Voltage (V_{IN})	8		36	V
Output Voltage (V_{OUT})	3.3		20	V
Output Current (I_{OUT})			3.5	A
Thermal Resistance from Junction to case (θ_{JC})		45		°C/W
Thermal Resistance from Junction to ambient (θ_{JA})		90		°C/W

Electrical Characteristics

T_J = 25℃ , V_{IN} = 12V , unless otherwise noted.

Characteristics	Symbol	Conditions	Min	Typ	Max	Units
Input Voltage	V_{IN}		7	-	38	V
UVLO Voltage	V_{UVLO_OFF}	VIN Rising	5.2	5.5	5.8	V
UVLO ON Voltage	V_{UVLO_ON}	VIN Falling	4	4.3	4.6	V
Input Over Voltage Protect	V_{OVP}			38		V
Quiescent Current	I_{CCQ}	VFB = 1.2V, No Switch	-	1300	-	μ A
Standby Current	I_{SB}	No Load	-	1.7	2.2	mA
FB Reference Voltage	V_{FB}		0.985	1	1.015	V
VFB Bias Current	I_{FB}				0.2	μ A
Current Sense AMP	V_{CS}	CSP-CSN	57	60	63	mV
Switching Frequency	F_{SW}	FS Floating	100	130	160	kHz
		Connect 470K Resister		300		kHz
FS Shut Down	V_{FSEN}			0.47		V
Maximum Duty Cycle				100	-	%
Minimum On-Time			-	250	-	ns
Current Limit	I_{LIM}		4.5			A
Vout Short Protect	V_{SCP}			3		V
Hiccup Interval	T_{HICCUP}			500		mS
Soft Start Time	T_{SS}			2		mS
RDSON of Power MOS	R_{DSON_H}	Temp=25°C		45		mΩ
	R_{DSON_L}	Temp=25°C		23		mΩ
Thermal Regulation	T_{TR}			150		°C
Thermal Shutdown Temp	T_{SD}		-	165	-	°C
Thermal Shutdown Hysteresis	T_{SH}		-	30	-	°C

Block Diagram



Operational Description

The NDP1435KC is a high efficiency, monolithic, synchronous step-down DC/DC converter utilizing a constant frequency, average current mode control architecture. Average current mode control enables fast and precise control of the output current. It operates through a wide VIN range and regulates with low quiescent current. An error amplifier compares the output voltage with an internal reference voltage of 1.0V and adjusts the peak inductor current accordingly. overvoltage and undervoltage comparators will turn off the regulator.

Main Control Loop

During normal operation, the internal top power switch (P-channel MOSFET) is turned on at the beginning of each clock cycle, causing the inductor current to increase. The sensed inductor current is then delivered to the average current amplifier, whose output is compared with a saw-tooth ramp. When the voltage exceeds the Vduty voltage, the PWM comparator trips and turns off the top power MOSFET. After the top power MOSFET turns off, the synchronous power switch (N-channel MOSFET) turns on, causing the inductor current to decrease. The bottom switch stays on until the beginning of the next clock cycle, unless the reverse current limit is reached and the reverse current comparator trips. In closedloop operation, the average current amplifier creates an average current loop that forces the average sensed current signal to be equal to the internal ITH voltage. Note that the DC gain and compensation of this average current loop is automatically adjusted to maintain an optimum current-loop response. The error amplifier adjusts the ITH voltage by comparing the divided-down output voltage (VFB) with a 1.0V reference voltage. If the load current changes, the error amplifier adjusts the average inductor current as needed to keep the output voltage in regulation.

Low Current Operation

The discontinuous-conduction modes (DCMs) are available to control the operation of the NDP1435KC at low currents. Burst Mode operation automatically switch from continuous operation to the Burst Mode operation when the load current is low.

VIN Overvoltage Protections

To protect the internal power MOSFET devices against transient voltage spikes, the NDP1435KC constantly monitors the VIN pin for an overvoltage condition. When VIN rises above 38V, the regulator suspends operation by shutting off both power MOSFETs. Once VIN drops below 37V, the regulator immediately resumes normal operation. The regulator executes its soft-start function when exiting an overvoltage condition.

Cable Drop Compensation

Due to the resistive of charger's output Cable, The NDP1435KC built in a simple user programmable cable voltage drop compensation using the impedance at the FB pin. Choose the proper resistance values for charger's output cable as show in this table:

R_{up} is the upper resistor the resistors divider net.

R_{low} is the lower resistor the resistors divider net.

R_{up}（K）	R_{low}（K）	Cable Drop compensation (mV)
100	25	130
160	39	200
360	91	500
470	120	680
820	200	1200
1200	300	1800

Frequency Selection and Shutdown

The switching frequency of the NDP1435KC can be programmed through an external resistor between 130kHz and 300 kHz， Floating this pin set the switching frequency to 130K, an external resistor can set the frequency up to 300kHz。 the switching frequency is set using the FS pins as shown in this table :

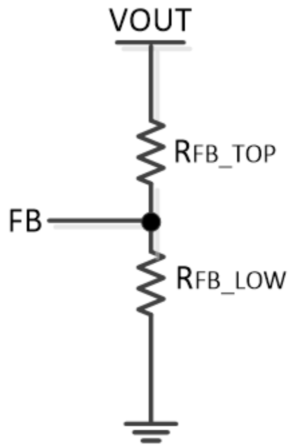
FS Resistor(KΩ)	Typ Frequency(kHz)
Floating	130
2000	180
1000	220
470	300

When the FS pin is below 0.3V, the NDP1435KC enters a low current shutdown state, reducing the DC supply current to 1.3mA.

Constant Voltage Output

NDP1435KC presets the VFB voltage to 1V. The Output can be set by extra resistance.

$$V_{OUT} = V_{FB} * \frac{R_{FB\_TOP} + R_{FB\_LOW}}{R_{FB\_LOW}}$$



Applications Information

Input Capacitor (C_{IN}) Selection

The input capacitance CIN is needed to filter the square wave current at the drain of the top power MOSFET. To prevent large voltage transients from occurring, a low ESR input capacitor sized for the maximum RMS current should be used. The maximum RMS current is given by:

$$I_{RMS} \cong I_{OUT(MAX)} \frac{V_{OUT}}{V_{IN}} \sqrt{\frac{V_{IN}}{V_{OUT}} - 1}$$

This formula has a maximum at VIN = 2VOUT, where: IRMS ≅ IOUT/2

This simple worst-case condition is commonly used for design because even significant deviations do not offer much relief. Note that ripple current ratings from capacitor manufacturers are often based on only 2000 hours of life which makes it advisable to further derate the capacitor, or choose a capacitor rated at a higher temperature than required. Several capacitors may also be paralleled to meet size or height requirements in the design. For low input voltage applications, sufficient bulk input capacitance is needed to minimize transient effects during output load changes.

Output Capacitor (C_{OUT}) Selection

The selection of COUT is determined by the effective series resistance (ESR) that is required to minimize voltage ripple and load step transients as well as the amount of bulk capacitance that is necessary to ensure that the control loop is stable. Loop stability can be checked by viewing the load transient response. The output ripple, △VOUT, is determined by:

$$\Delta V_{OUT} < \Delta I_L \left(\frac{1}{8 \bullet f \bullet C_{OUT}} + ESR \right)$$

The output ripple is highest at maximum input voltage since △IL increases with input voltage. Multiple capacitors placed in parallel may be needed to meet the ESR and RMS current handling requirements. Dry tantalum, special polymer, aluminum electrolytic, and ceramic capacitors are all available in surface mount packages. Special polymer capacitors are very low ESR but have lower capacitance density than other types. Tantalum capacitors have the highest capacitance density but it is important to only use types that have been surge tested for use in switching power supplies. Aluminum electrolytic capacitors have significantly higher ESR,but can be used in cost-sensitive applications provided that consideration is given to ripple current ratings and long-term reliability. Ceramic capacitors have excellent low ESR characteristics and small footprints.

Inductor Selection

Given the desired input and output voltages, the inductor value and operating frequency determine the ripple current:

$$\Delta I_L = \frac{V_{OUT}}{F * L} \left(1 - \frac{V_{OUT}}{V_{IN(MAX)}} \right)$$

Lower ripple current reduces power losses in the inductor, ESR losses in the output capacitors and output voltage ripple. Highest efficiency operation is obtained at low frequency with small ripple current. However, achieving this requires a large inductor. There is a trade-off between component size, efficiency and operating frequency. A reasonable starting point is to choose a ripple current that is about 40% of I_{OUT}(MAX). To guarantee that ripple current does not exceed a specified maximum, the inductance should be chosen according to:

$$L = \frac{V_{OUT}}{F * \Delta I_{L(MAX)}} \left(1 - \frac{V_{OUT}}{V_{IN(MAX)}} \right)$$

Once the value for L is known, the type of inductor must be selected. Actual core loss is independent of core size for a fixed inductor value, but is very dependent on the inductance selected. As the inductance or frequency increases, core losses decrease. Unfortunately, increased inductance requires more turns of wire and therefore copper losses will increase. Copper losses also increase as frequency increases Ferrite designs have very low core losses and are preferred at high switching frequencies, so design goals can concentrate on copper loss and preventing saturation. Ferrite core material saturates "hard", which means that inductance collapses abruptly when the peak design current is exceeded. This results in an abrupt increase in inductor ripple current and consequent output voltage ripple. Do not allow the core to saturate!

Different core materials and shapes will change the size/current and price/current relationship of an inductor. Toroid or shielded pot cores in ferrite or permalloy materials are small and don't radiate much energy, but generally cost more than powdered iron core inductors with similar characteristics. The choice of which style inductor to use mainly depends on the price versus size requirements and any radiated field/EMI requirements. New designs for surface mount inductors are available from Coilcraft, Toko, Vishay, NEC/Tokin, TDK and Würth Electronik.

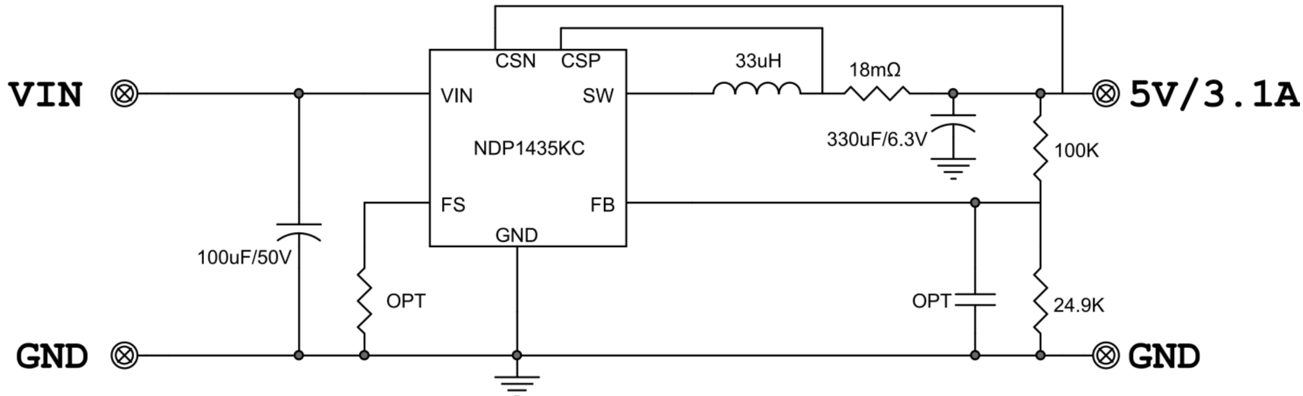
Efficiency Considerations

The percent efficiency of a switching regulator is equal to the output power divided by the input power times 100%. It is often useful to analyze individual losses to determine what is limiting the efficiency and which change would produce the most improvement. Percent efficiency can be expressed as: % Efficiency = 100% – (Loss1 + Loss2 + …) where Loss1, Loss2, etc. are the individual losses as a percentage of input power. Although all dissipative elements in the circuit produce losses, three main sources usually account for most of the losses in NDP1435KC circuits: 1) I2R losses, 2) switching and biasing losses, 3) other losses.

Thermal Conditions

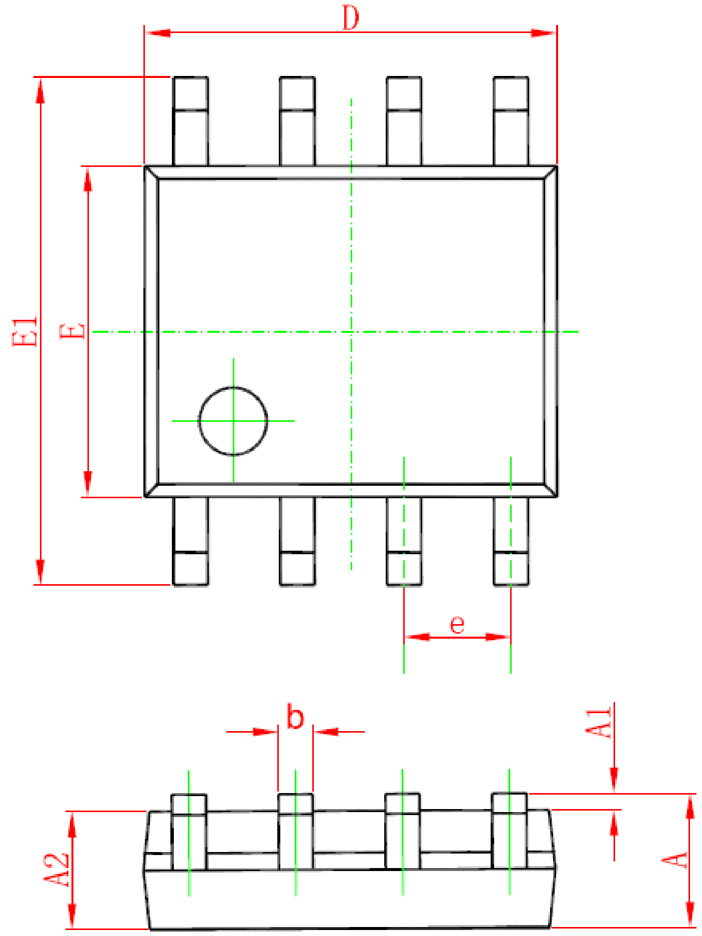
In most applications, the NDP1435KC does not dissipate much heat due to its high efficiency and low thermal resistance. However, in applications where the NDP1435KC is running at high ambient temperature, high VIN, and maximum output current load, the heat dissipated may exceed the maximum junction temperature of the part. If the junction temperature reaches approximately 165°C, both power switches will be turned off until the temperature drops about 30°C cooler to avoid the NDP1435KC from exceeding the maximum junction temperature, the user will need to do some thermal analysis. The goal of the thermal analysis is to determine whether the power dissipated exceeds the maximum junction temperature of the part. If the application calls for a higher ambient temperature and/or higher switching frequency, care should be taken to reduce the temperature rise of the part by using a heat sink or forced air flow.

Typical Applications



Package Outline Drawing

8-Lead Standard Small Outline Package [SOP-8]



Symbol	Dimensions In Millimeters		Dimensions In Inches	
	Min	Max	Min	Max
A	1.350	1.750	0.053	0.069
A1	0.050	0.250	0.002	0.010
A2	1.250	1.650	0.049	0.065
b	0.310	0.510	0.012	0.020
c	0.170	0.250	0.006	0.010
D	4.700	5.150	0.185	0.203
E	3.800	4.000	0.15	0.157
E1	5.800	6.200	0.228	0.244
e	1.270 (BSC)		0.05 (BSC)	
L	0.400	1.270	0.016	0.050
θ	0º	8º	0º	8º

Notes

1. Use millimeters as the primary measurement
2. Dimensioning and tolerances conform to ASME Y14.5M. – 1994
3. These dimensions do not include mold flash or protrusions.
4. Mold flash or protrusions shall not exceed 0.15mm

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